



Thyristor Based DC Motor Control with Improved PF & THD

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Abstract: DC motors are widely used in industries because of its versatile characteristics and because of power electronics devices its controlling is becoming sophisticated and precise, but on the other hand because of the power electronics devices power factor and total harmonics distortion problem is becoming more prominent. In this paper DC motor control methodology is proposed which includes thyristor based converters but with improved power factor and total harmonics distortion.

Keywords: AC/DC converter, DC motor, Power Factor, Speed control, Total Harmonic Distortion.

1. Introduction

Because of low cost, less complex control structure and wide range of speed and torque, DC motor are popular in industry. Available methods of speed control of DC drives are field control, armature control and armature resistance control methods [1]. Speed of a DC motor can be controlled easily in both the ranges above and below the base speed. Most of the time, DC motors are customized at the time of installation as per the need which makes them irreplaceable. Armature voltage control method of speed control of DC drive is popularly used in which controlled rectifier or chopper are involved, though due to power electronics elements, an undesirable nonlinear torque speed characteristics are observed [2].

In past, many researchers worked on various converter topologies of DC motor control for different industrial applications [5, 6, 7, 8, 9], but all of them are thyristor based. For simulation of various topologies MATLAB with its tool boxes like Simulink and SimPowerSystem are used [3, 7].

2. Mathematical modelling of DC motor

To analyse the torque speed characteristics, power factor and total harmonics distortion, the dynamic and steady-state model of separately excited DC motor is required. Figure 1 shows the schematic representation of the model of a separately excited DC motor, in which e_a is the terminal voltage applied to the motor, R_a and L_a are the resistance, and inductance of the armature circuit respectively, R_f and L_f are the resistance, and inductance of the field circuit respectively, e_b is generated back emf and T_m is the electromagnetic torque developed by the motor. The related DC Motor parameters are mentioned in appendix A.

Due to the interaction of field flux with current in armature conductors, the torque is produced which is given by Eq. (1)

$$T_m = K_t \phi i_a \quad (1)$$

Here K_t is a constant depending on motor windings and geometry and ϕ is the flux per pole due to the field winding. The direction of armature current decides the direction of the

torque produced. When armature rotates, the flux linking the armature winding will vary with time and therefore according to Faraday's law, an emf will be induced across the winding. This generated emf, known as the back emf, depends on speed of rotation as well as on the flux produced by the field and given by Eq. (2)

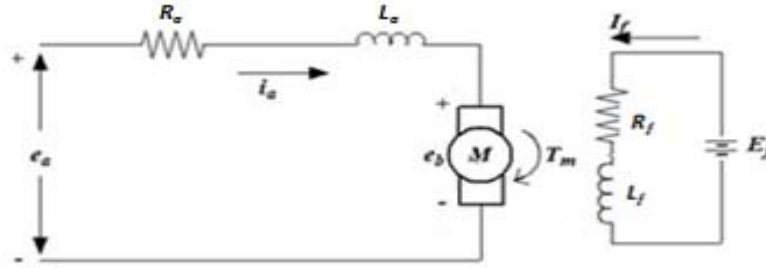


Figure 1. Equivalent circuit of separately excited DC motor

$$e_b = K_t \phi \omega \quad (2)$$

By applying KVL at input side of in figure 1,

$$e_a = i_a R_a + L_a \frac{di_a}{dt} + e_b \quad (3)$$

In steady state condition,

$$E_a = I_a R_a + E_b \quad (4)$$

In terms of torque and speed, the steady state equation will be given by Eq. (5)

$$E_a = \frac{T_m}{K_t \phi} R_a + K_t \omega \phi \quad (5)$$

So,

$$\omega = \frac{E_a}{K_t \phi} - \frac{T_m}{(K_t \phi)^2} R_a \quad (6)$$

Thus from the above equation it is clear that speed can be controlled by varying three parameters, namely E_a , R_a , and ϕ . The three methods of speed control are following:

- Armature voltage controlled (E_a).
- Armature resistance controlled (R_a).
- Flux controlled (ϕ).

Adding external resistor to the DC drive to control the speed of DC motor is not a healthy practice as large part of energy get loosed in terms of heat due to the external resistor R_{ext} . Armature voltage controlled is preferred for speed up to rated speed (base speed), and flux control for speed beyond rated speed but at the same time the maximum torque capability of the motor is reduced since for a given maximum armature current, the flux is less than the rated value and so as the maximum torque produced is less than the maximum rated torque [4].

Figure 2 illustrate the ideal torque speed characteristic which reflects equation (6), using armature voltage control method in which the voltage applied across the armature e_a is varied keeping field voltage constant [10].

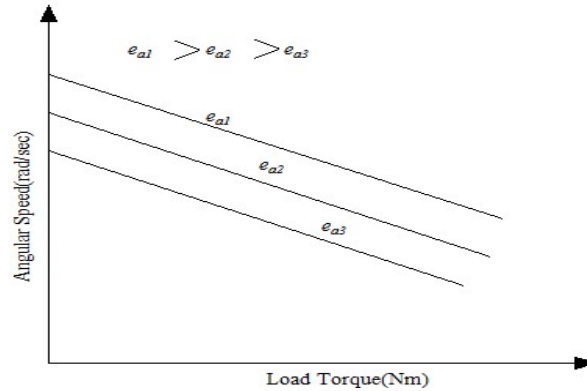


Figure 2. Torque speed characteristics of the separately excited DC motor at different armature voltages

3. Thyristor based techniques of DC motor speed control

Figure 3 shows a separately excited DC motor fed through single phase half wave converter. It offers only one quadrant drive. Such type of drives, are used up to about 0.5 kW DC motor.

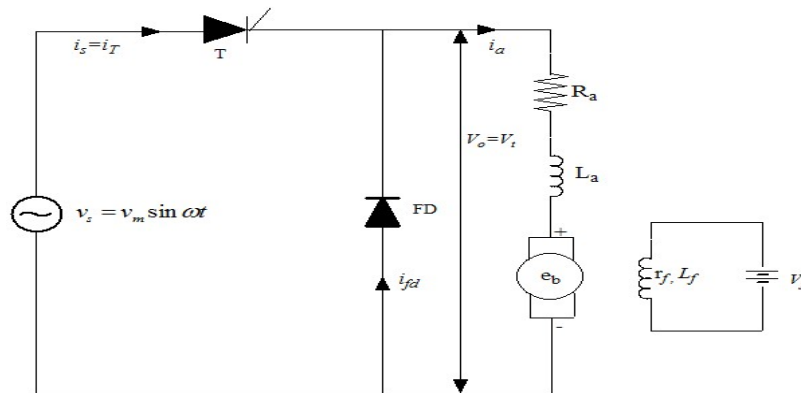


Figure 3. Single phase half wave converter drive

For single phase half wave converter, average output voltage of converter can be calculated as, given by Eq. (7)

$$V_0 = \frac{V_m}{2\pi}(1 + \cos \alpha), \text{ for } 0 < \alpha < \pi \quad (7)$$

An ideal DC source is preferred over half wave converter for field circuit of half wave converter drive otherwise the magnetic losses of the motor increase due to high ripple content in the field excitation current. A separately excited DC motor fed through single phase semiconverter is shown in figure 4. This converter also offer only one quadrant drive and is used up to 15 kW DC drives.

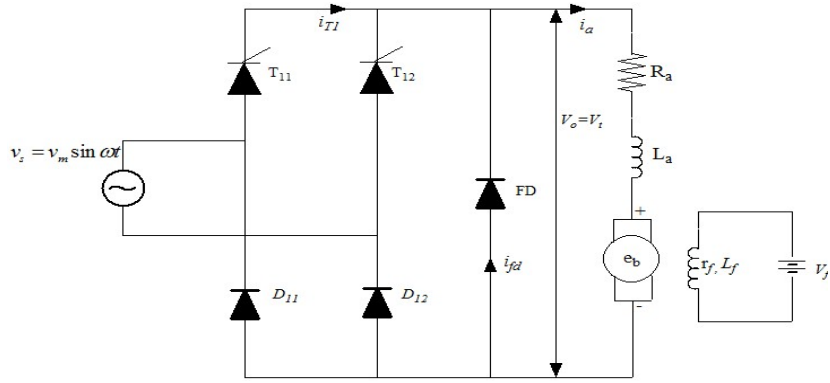


Figure 4. Single phase semi converter drive

With a single phase semiconverter in the armature circuit, equation (8) gives the average armature voltage as,

$$V_0 = V_t = \frac{V_m}{\pi}(1 + \cos \alpha), \text{ for } 0 < \alpha < \pi \quad (8)$$

A single phase full converter drive offers a two quadrant drive operation and is limited to applications up to 15kW, which is shown in figure 5. The armature converter gives $+V_o$ or $-V_o$ and allows operation in the first and fourth quadrant. The converter in the field circuit could be semi, full or even dual converter. The reversal of the armature or field voltage allows operation in the second and third quadrant.

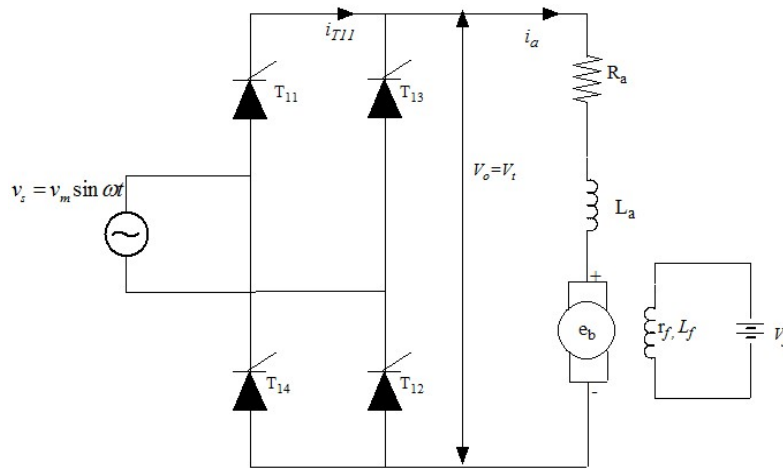


Figure 5. Single phase full converter drive

The average armature voltage in armature circuit for single phase full converter drive is given by Eq. (9)

$$V_0 = V_t = \frac{2V_m}{\pi}(1 + \cos \alpha), \text{ for } 0 < \alpha < \pi \quad (9)$$

To realize single phase dual converter, two single phase full converters are connected as shown in figure 6.

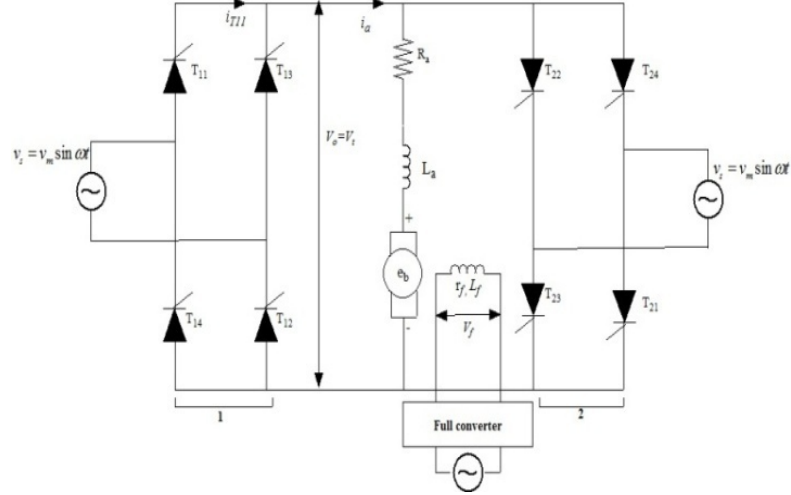


Figure 6. Single phase dual converter drive

In figure 6, there are two single phase full wave converters either converter 1 operates to supply a positive armature voltage V_o , or converter 2 operates to supply negative armature voltage $-V_o$. Converter 1 provides operation in first and fourth quadrants, and converter 2 provides operation in second and third quadrants. It is four quadrant drive and provides four modes of operation: forward powering, forward braking (regeneration), reverse powering, and reverse braking (regeneration). The field converter could be a full wave converter, a semiconverter, or a dual converter.

If converter 1 operates at a firing angle of α_1 then equation (10) gives the armature voltage as,

$$V_o = V_t = \frac{V_m}{\pi}(1 + \cos \alpha_1), \text{ for } 0 < \alpha < \pi \quad (10)$$

And similarly, if converter 2 operates at a firing angle of α_2 then equation (11) gives the armature voltage as, [11].

$$V_o = V_t = \frac{V_m}{\pi}(1 + \cos \alpha_2) \quad (11)$$

4. Methodology

Harmonics puts very adverse effects on the power system, the biggest problem with harmonics is voltage waveform distortion. The relation can be deduced between the fundamental and distorted waveforms by mathematical tool Fast Fourier Transform (FFT), in which the square root of the sum of squares of all harmonics generated by load is found out and then that number is divided by the nominal frequency. Using FFT, total harmonic distortion (THD) contained by the nonlinear current or voltage waveform is determined. Harmonics can cause overloading and overheating of load which can result in load failure.

Rectifier is the main component of any power system based system. The input stage of any AC-DC converter comprise of a full-bridge rectifier followed by a large filter capacitor. The input current of such a rectifier circuit comprises of large discontinuous peak current pulses that result in high input current harmonic distortion. The high distortion of the input current occurs due to the fact that the diode rectifiers conduct only for a short period. This period

corresponds to the time when the mains instantaneous voltage is greater than the capacitor voltage. Since the instantaneous mains voltage is greater than the capacitor voltage only for very short period of time, when the capacitor is fully charged, large current pulses are drawn from the line during this short period of time and that will lead to poor power factor. So from above discussion it can be concluded that if the shape of input current or voltage can be maintained as a sinusoidal wave, the power factor and total harmonic distortion (THD) both can be improved.

Many input current wave shaping methods have been proposed to overcome disadvantages of conventional rectifiers like high input current harmonic components, low power factor, low rectifier efficiency etc. Those wave shaping method can be broadly classified as active, passive and hybrid methods. In the past, designers have used three passive wave shaping methods to improve the input power factor and reduce total harmonic distortion THD of conventional ac-to-dc rectifiers which are Input passive filter method, resonant passive input filters method and Ferro resonant transformer method. [12]

Among the passive wave shaping methods proposed earlier, the novel method proposed in 1990 is superior to others in reducing the input current harmonics and improving the input power factor [13]. The novel method can efficiently improve the power factor, however, the further improvement of the input power factor is difficult to be achieved, and the input current's total harmonic distortion is still high, which is the main disadvantage of the novel topology. This novel method uses an input parallel resonant tank of capacitor and inductor to remove the third harmonic component from the input current. The input power factor increases because the third harmonic component is the main reason of the low input power factor. The advantages of the this method over the conventional method include: (i) low input current THD (ii) higher input power factor, and (iii) increase in the efficiency of the rectifier. Fig. 7 shows the block diagram how the wave shaping method is used to improve the power factor and total harmonic distortion of DC drives.

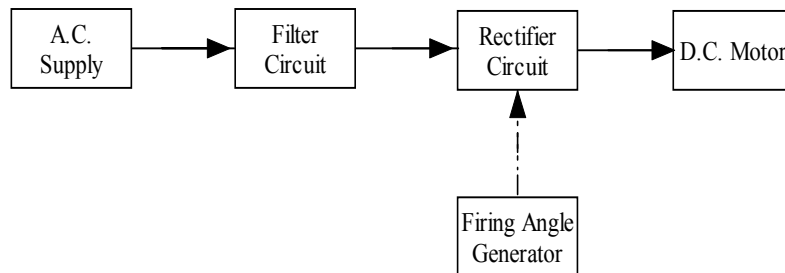


Figure 7. Block diagram of methodology used

5. Simulation Results

Some assumptions were made to analyze the circuits which are the following:-

- Ideal filter components.
- The forward voltage drop and reverse leakage current of diodes are neglected.

Five different passive power factor improvement topologies for low power output with 220volt/50 Hz ac input have been considered.

The five different topologies are:-

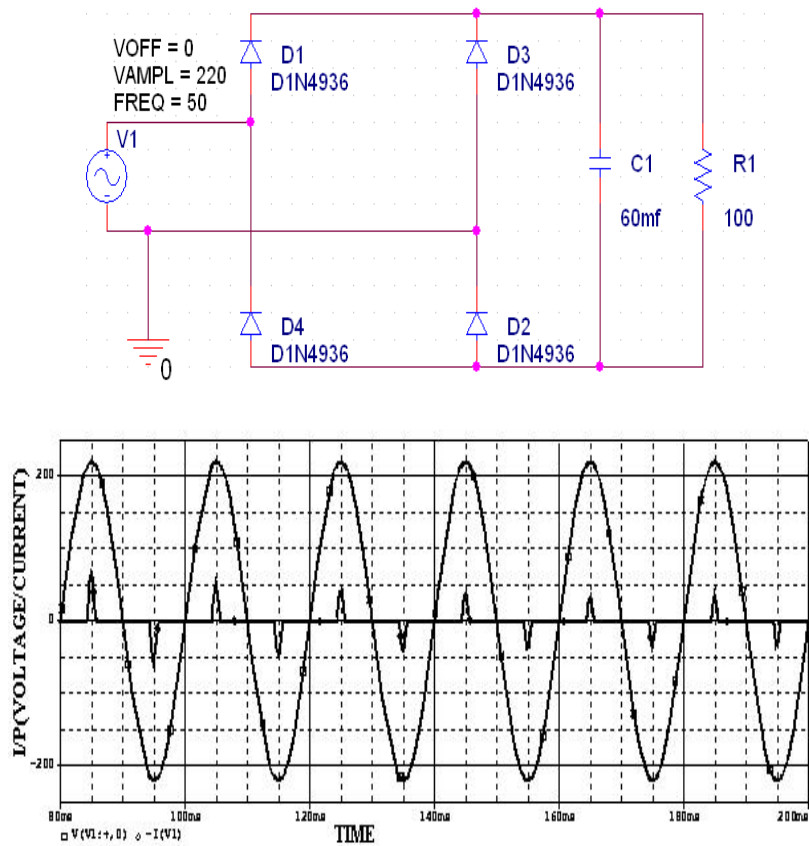
1. Conventional single phase diode rectifier with filter capacitor.
2. Single phase diode rectifier with LC filter.
3. Single phase diode rectifier circuit with parallel input resonant filter.
4. Single phase diode rectifier circuit with series input resonant filter.

5. Single phase diode rectifier circuit with improved parallel input resonant filter. Table 1 shows the specifications of the components used in the topologies.

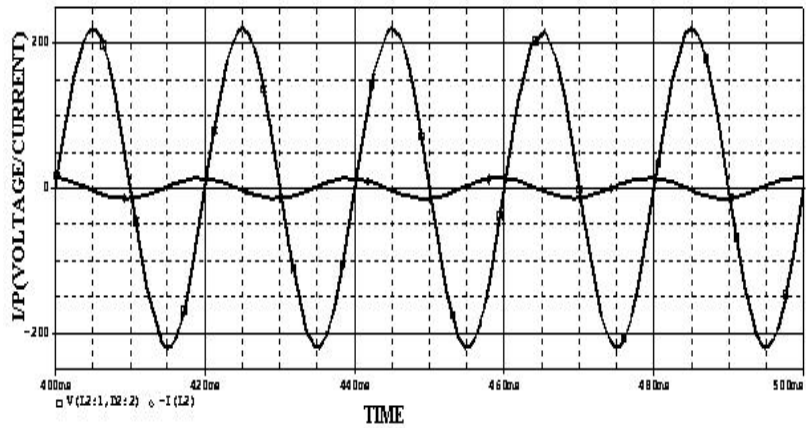
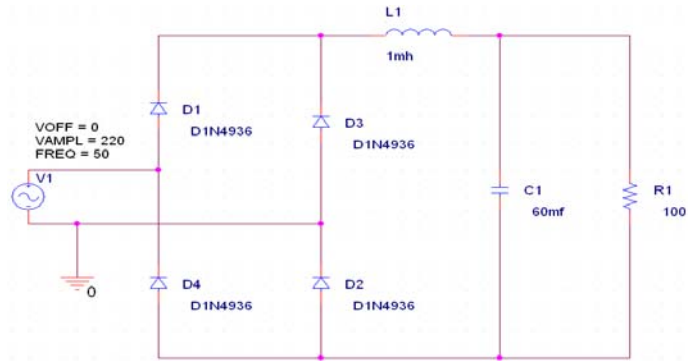
Table 1. Specification of the components

Components	Specifications
AC supply	220V/50Hz
Diodes	DIN4936
Resistances	100Ω
Capacitors	60mF/0.1mF/100mF/500μF
Inductor	1mH/50mH/5mH/.005mH

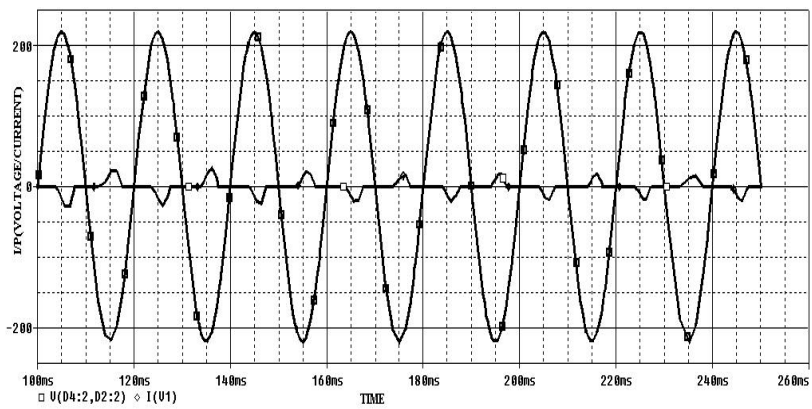
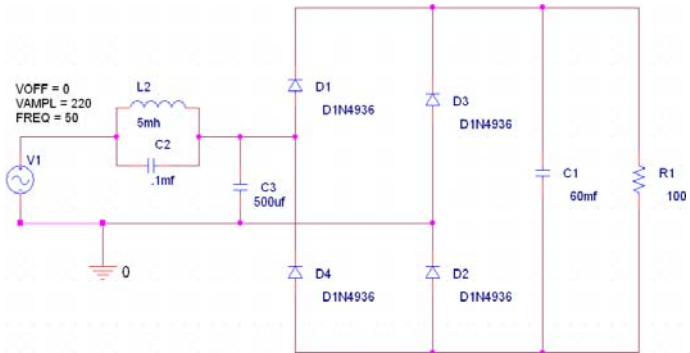
Figure 8 shows the simulation prototype of different passive power factor improvement topologies with their respective input current and voltage waveform.



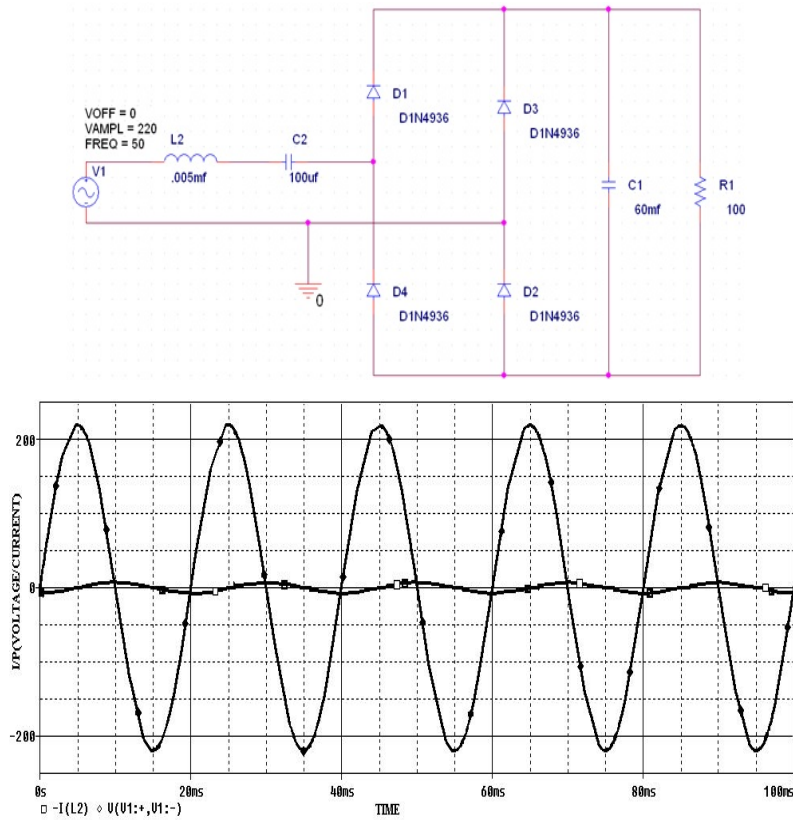
(a).



(b).



(c).



(d).

Figure 8(a) shows the simulated prototype of a conventional single phase diode rectifier with filter capacitor, in which the harmonics of input current, which are highly undesirable, are seen. The output filter capacitor value (C_1) is calculated using eq. 13.

$$C_1 = \frac{1}{4fR} \left[1 + \frac{1}{\sqrt{2RF}} \right] \quad (13)$$

RF :- ripple factor

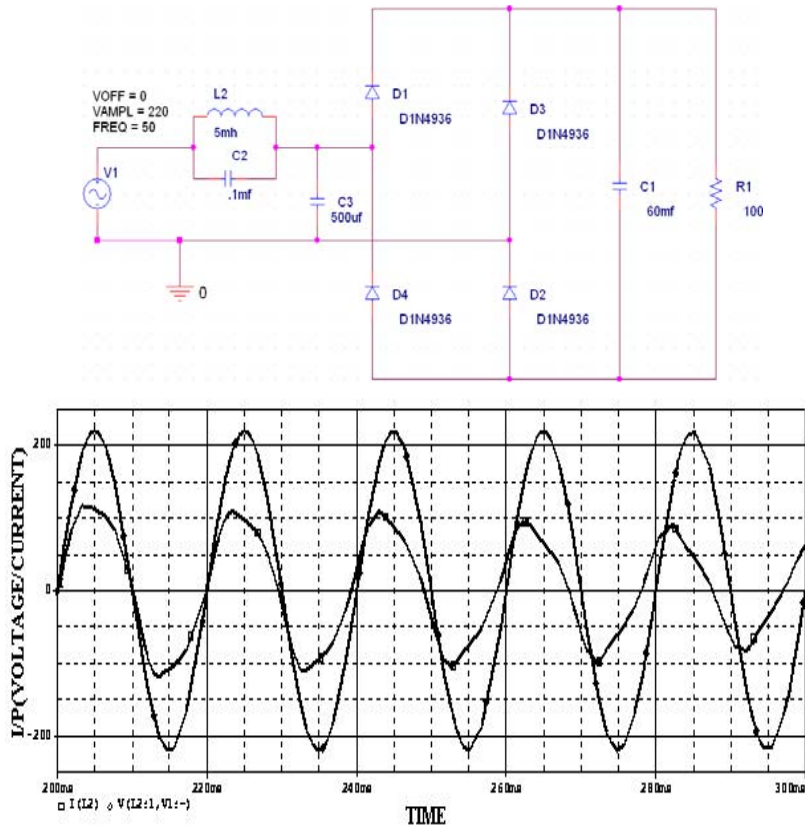
RR :- output resistance

f :- frequency of ac source

To get minimum ripple factor we have chosen $C_1=60$ mF (milli farads).

Figure 8(b) shows the simulated prototype of a conventional single phase diode rectifier with LC filter. The inclusion of the inductor results in larger conduction angle of the current pulse and reduced peak and r.m.s values, and the waveform of input current and input voltage show that the harmonics of input current are reduced.

For low values of inductance the input current is discontinuous and pulsating. However, it is shown [14] that even for infinite value of the inductance, the PF cannot exceed 0.9 for this kind of arrangement.



(e).

Figure 8. Simulation prototype of various filter circuit with their I/P voltage and current waveform

- (a). Single phase diode rectifier with filter capacitor
- (b). Single phase diode rectifier with LC filter
- (c). Single phase diode rectifier with parallel input resonant filter
- (d). Single phase diode rectifier with series input resonant filter
- (e). Single phase diode rectifier with improved parallel input resonant filter

Figure 8(c) shows the simulated prototype of single phase diode rectifier using parallel resonant circuit and input current and voltage waveform, which shows the prominent improvement in the harmonics and the value of inductor and capacitor for this topology are calculated using the analysis discussed below.

The n^{th} harmonic component of the equivalent impedance of the input parallel resonant filter is given by eq. 14.

$$Z_n = \frac{nX_{L_2} * \frac{X_{C_2}}{n}}{jnX_{L_2} - j\frac{X_{C_2}}{n}} \quad (14)$$

X_{L_2} is impedance of input resonant inductor L at fundamental frequency.

X_{C_2} is impedance of input resonant capacitor C at fundamental frequency.

The third harmonic impedance of the input resonant filter will be infinity (theoretically).

Therefore,

$$3X_{L_2} = \frac{X_{C_2}}{3}$$

and

$$L_2 = \frac{1}{9\omega^2 C_2}$$

Where $\omega = 2\pi f$ and is f in Hz.

Figure 8(d) the simulated prototype of a single phase diode rectifier with series input resonant filter with its input voltage and current waveform is shown in fig. 8(d). The values of inductor and capacitor considered in the prototype are calculated using the analysis discussed below. For a series resonant filter at the input end of a single phase rectifier, the capacitance C_2 and L_2 is chosen such that the resonance condition is satisfied, and the minimum ripple is achieved.

$$\omega = \frac{1}{\sqrt{L_2 C_2}} \quad (15)$$

Where $\omega = 2\pi f$ and f is in Hz

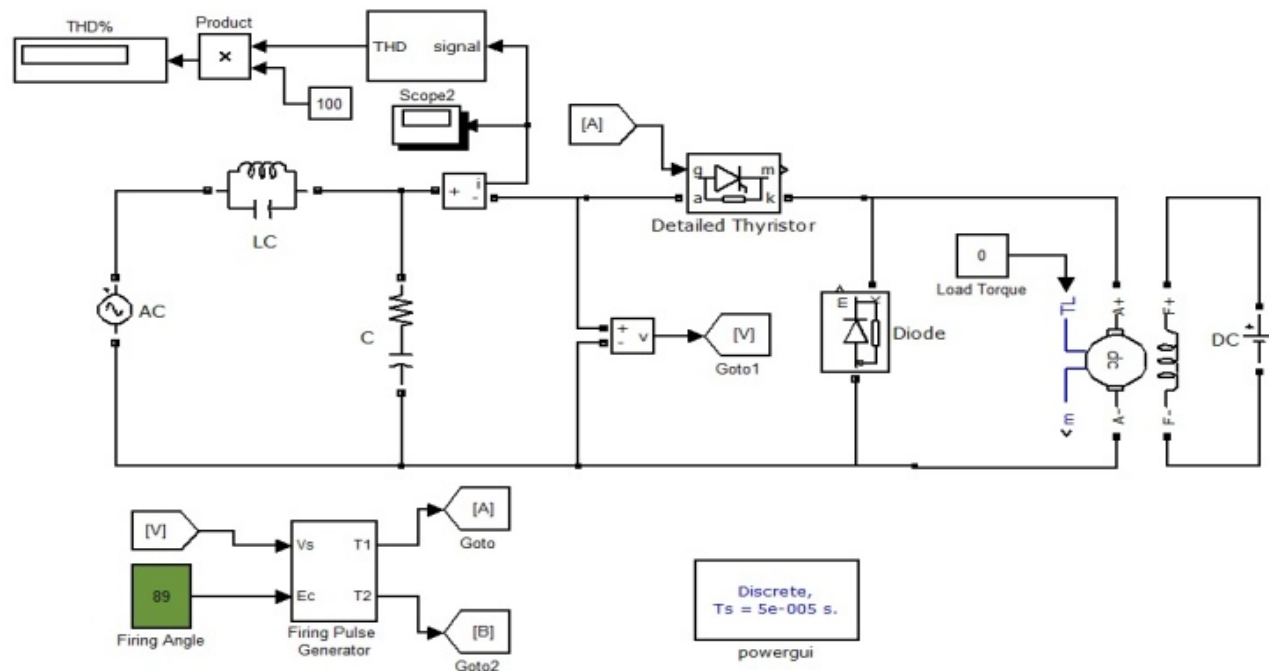
Figure 8(e) shows the simulated prototype of a proposed single phase diode rectifier circuit with improved parallel input resonant filter with its input current and voltage waveform, for which values of C_3 are chosen ranging from 100 μ f(micro farads) to 1mf(milli farads) and is selected such that the input power factor at rated output power reaches its peak value.

Table 2 shows the calculated parameters for single phase diode rectifier circuit with various filter topologies in tabulated form, which shows improved parallel input resonant filter topology performs well amongst other topologies for which power factor is 0.931 and total harmonic distortion reduced to 5.591.

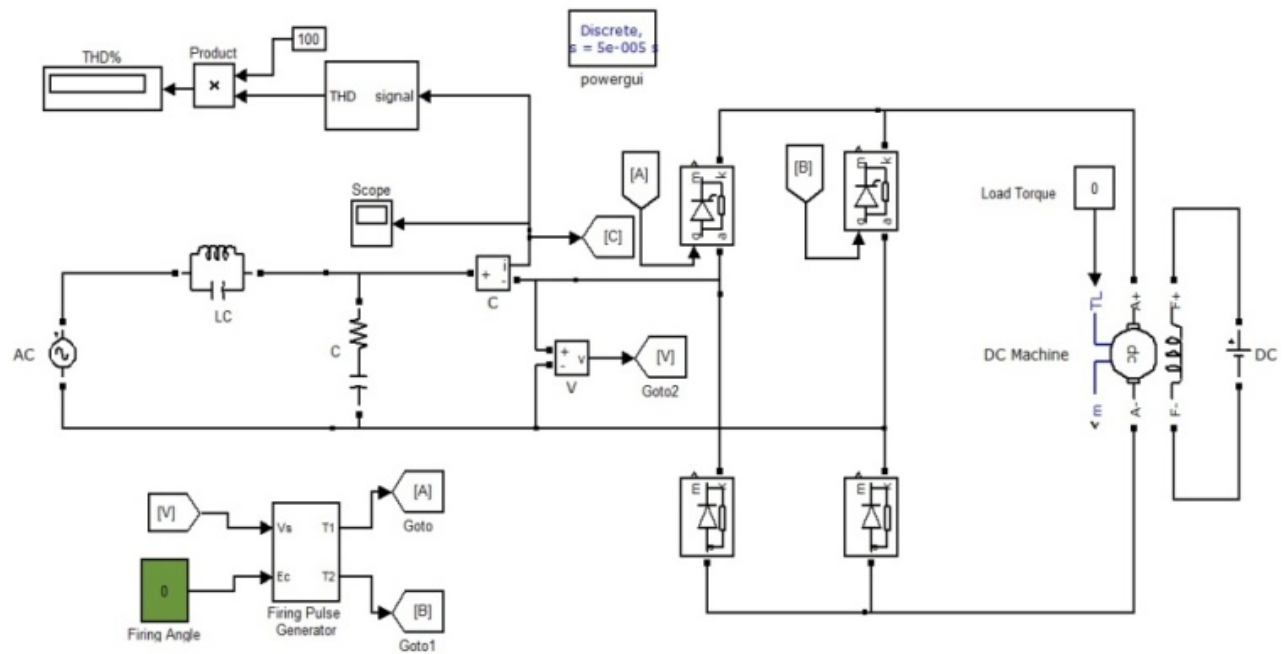
Table 2. Parameters for various filter topologies

Type of Filter /Parameters	PF	DF	CDF	HF	% THD
Single phase diode rectifier with filter capacitor	0.215	0.999	0.215	4.527	176.9
Single phase diode rectifier with LC filter	0.3629	0.967	0.375	2.471	84.09
Single phase diode rectifier with parallel input resonant filter	0.592	0.919	0.644	1.186	23.39
Single phase diode rectifier with series input resonant filter	0.64	0.953	0.679	1.08	10.12
Single phase diode rectifier with improved parallel input resonant filter	0.931	0.99	0.94	0.36	5.591

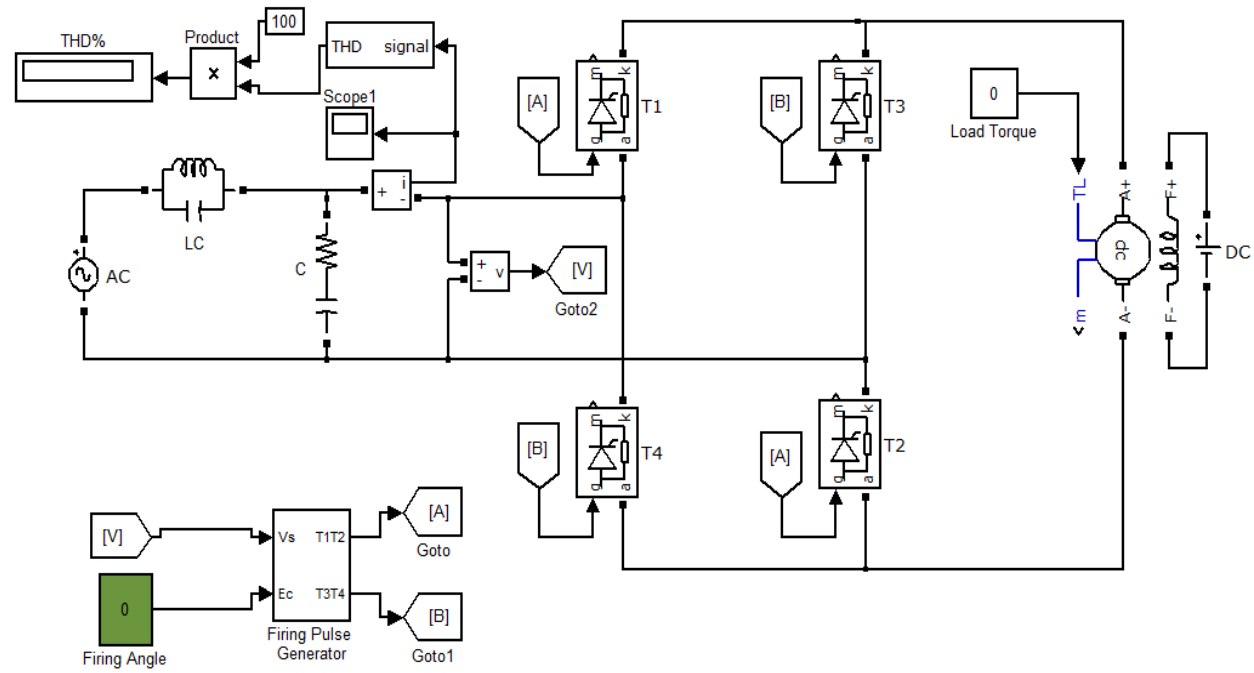
It can be concluded from table 2 that improved parallel resonant filter topology gives the best result in terms of power factor and total harmonic distortion, so a simulation model of the same topology with different converter drives are described in section III, which are shown in figure 9.



(a).



(b).



(c).

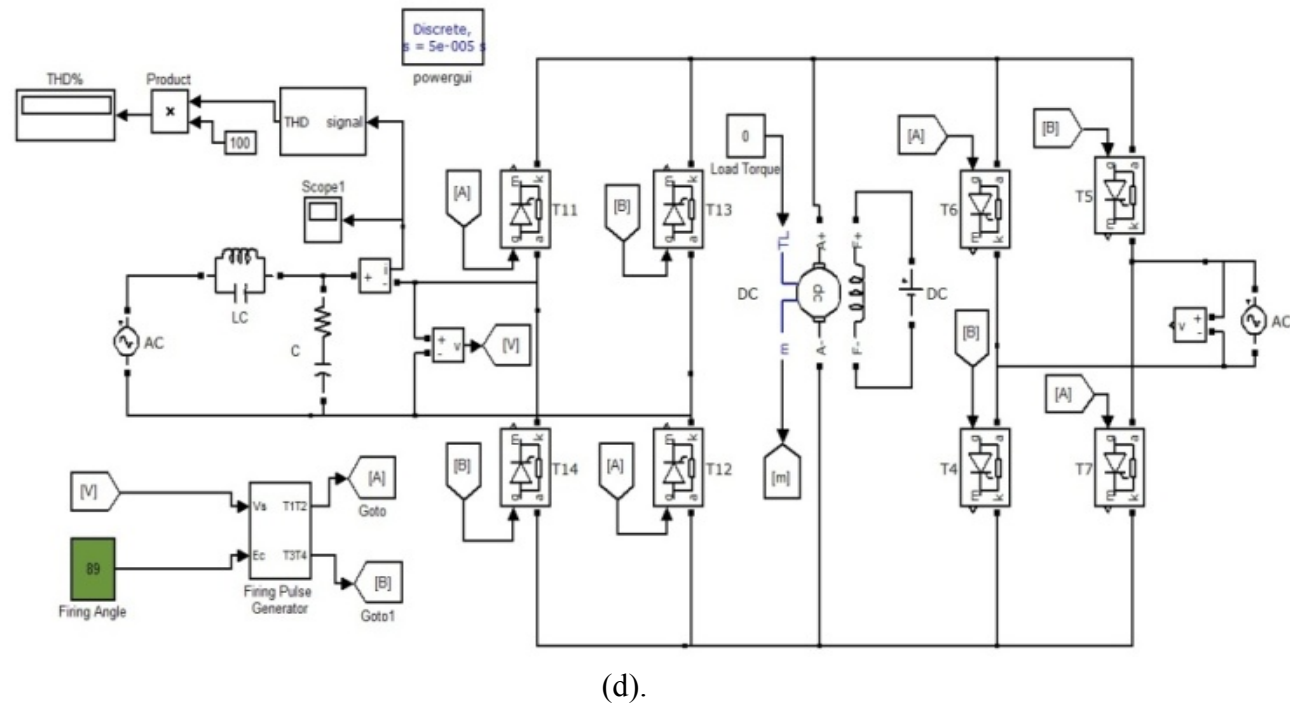


Figure 9. Converter drives with PFC circuit

- (a) Half wave converter drive
- (b) Semiconverter drive
- (c) Full converter drive
- (d) Dual converter drive

Table 7 and 8 shows the value of power factor, improved power factor, total harmonic distortion with improved total harmonic distortion for different type of converter drives at firing angle 89°.

Table 7. Comparison of PF for different drives

Type of drive	Firing angle	PF	Improved PF	% improvement in PF
Half wave converter drive	89	0.42	0.78	85
Semi converter drive	89	0.43	0.71	65
Full wave converter drive	89	0.37	0.68	83
Dual converter drive	89	0.61	0.99	62

Table 8. Comparison of % THD for different drives

Type of drive	Firing angle	% THD	Improved %THD	% Improvement in THD
Half wave converter drive	89	104.8	11.24	89
Semi converter drive	89	56	4.08	92
Full wave converter drive	89	38.96	3.6	90
Dual converter drive	89	65	10.73	84

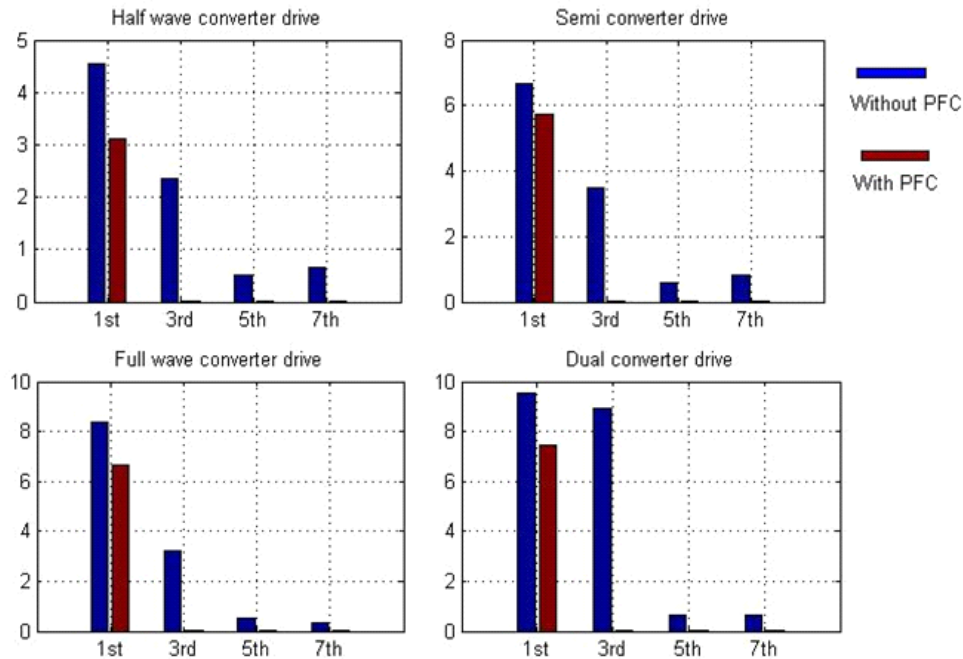


Figure 10. Current harmonics for different drives

Figure 10 shows the input current harmonics (odd) with and without power factor correction, and Table 9 shows the percentage reduction in current harmonics for different drives, which shows a remarkable reduction in 3rd harmonics for which the power factor correction circuits are designed.

Table 9. Comparison of current harmonics for different drives

Type of drive	Percentage reduction in current harmonics			
	1 st	3 rd	5 th	7 th
Half wave converter drive	31.78022	99.98306	99.23547	99.40972
Semi converter drive	14.00843	99.93974	99.46487	99.4283
Full wave converter drive	20.90725	99.98124	99.66041	99.11196
Dual converter drive	21.8589	99.95297	99.79256	99.57109

6. Conclusions

In the above discussion, five types of power factor improvement topologies are implemented and their performance is compared on the basis of five parameters those are power factor, input current distortion factor, input current harmonic factor, input displacement factor and total harmonic distortion, and it is found that the single phase diode rectifier circuit with improved parallel input resonant filter performs well. Thus the same parallel input resonant filter is applied with different types of DC drives systems which are single phase half wave converter drive, single phase semiconverter drive, single phase full converter drive and single phase dual converter drive, and a significant improvement of 85% for half wave converter drive, 65% for semi converter drive, 83% for full converter drive and 63% for dual converter drive in power factor is observed and similarly in total harmonic distortion percentage improvement is 89%, 92%, 90%, and 84% respectively.

But selection of filter components still involves complex mathematical calculations, so the selection of components can be done by applying artificial intelligence.

APPENDIX A

The parameters of separately excited DC motor

Rated Power (P)	5 Hp
Rated Armature Voltage	240 V
Armature Resistance R_a	2.518 Ω
Armature Inductance L_a	0.028 H
Field Resistance R_f	281.3 Ω
Field Inductance L_f	156 H
Rated Speed	1750 RPM
Rated Field Voltage	300 V

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